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If no title is shown please refer to the description.
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System, receiver and method of operation for spread OFDM wireless communication

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SYSTEM, RECEIVER AND METHOD OF OPERATION FOR SPREAD OFDM WIRELESS COMMUNICATION

Field of the Invention

This invention relates to multicarrier wireless communication systems, and more specifically Orthogonal Frequency Division Multiplex (OFDM) modulation schemes.

Background of the Invention

Such modulation schemes are now widely used in standards as a means to provide high data rates for communication systems including wireless local area networks (WLANs): 'IEEE 802.11a' in USA and 'HIPERLAN/2' in Europe, ADSL (Asynchromous Digital Subscriber Line) over twisted pairs and 'HomePLUG' on powerlines.

For the next decade, the challenge is to deliver an increased data rate coping with the requirements of multimedia broadband transmissions. None of the existing standards will be able to meet these requirements on a larger scale (involving many users) which motivates the search for more robust yet simple modulation schemes that, combined with an appropriate decoding algorithm, show better performance in terms of Packet Error Rate (PER) than classical OFDM systems. This technical criterion translates directly into increased system throughput (rather then capacity). Clearly, an attractive property for such a new modulation scheme would be for it

to be viewed as a simple extension of OFDM so that it could be implemented in existing standards as a proprietary transmission mode. In this way it could also provide a means for smooth transition to new standards.

In the field of this invention, enhancements have been proposed as a workaround for alleviating an inherent OFDM weakness: when a carrier is subject to a strong channel attenuation, even in absence of noise, the data conveyed is irremediably lost. The classical alternative is to use forward error correction (FEC) coding to spread the information along the carriers, but another strategy has been proposed: to combine the strength of OFDM and CDMA by pre-processing the block of symbols to be transmitted by a unitary spreading matrix $\mathbf{W}$ (often chosen to be a Walsh Hadamard transform for its attractive implementation properties) prior to the FFT/IFFT (Fast Fourier Transform/Inverse FFT) modulation.

This redundantless precoder $\mathbf{W}$ has the role of uniformly spreading the information to be transmitted on all the carriers so that even if one carrier is unrecoverable, the information transmitted can still be retrieved by decoding of other subbands.

Implementations of such spread OFDM (SOFDM also known as single user OFDM-CDMA with cyclic prefix) modulation techniques require successive interference cancellation (SIC), and many SIC algorithms have been proposed. One of the most well known is 'V-BLAST' proposed by Bell Labs for multiple antennas systems in the publication by G.J. Foschini and M.J. Gans, "On Limits of Wireless

Communications in a fading Environment when Using Multiple Antennas", *Wireless Personnal Communications* 6:311-335, 1998. However, it has been demonstrated (in the publication by P. Loubaton, M. Debbah and M. de Courville, "Spread OFDM Performance with MMSE Equalization", in *International Conference on Acoustics, Speech, and Signal Processing*, Salt Lake City, USA, May 2001) that V-BLAST algorithms are not suited for conventional SOFDM systems due to the averaging of the SNRs (signal/noise ratios) at the receiver across the carriers during the despreading step. Moreover, such approaches lead to a tremendous decoding complexity due to the computation of several pseudo inverse matrices.

A need therefore exists for an OFDM communication system and decoding algorithm for use therein wherein the abovementioned disadvantage(s) may be alleviated.

Statement of Invention

In accordance with a first aspect of the present invention there is provided a spread OFDM wireless communication system as claimed in claim 1.

In accordance with a second aspect of the present invention there is provided a spread OFDM wireless communication system as claimed in claim 7.

In accordance with a third aspect of the present invention there is provided a receiver, for use in a

spread OFDM wireless communication system, as claimed in claim 8.

In accordance with a fourth aspect of the present invention there is provided a receiver, for use in a spread OFDM wireless communication system, as claimed in claim 13.

In accordance with a fifth aspect of the present invention there is provided a method, of operating a receiver in a spread OFDM wireless communication receiver, as claimed in claim 14.

In accordance with a sixth aspect of the present invention there is provided a method, for performing minimum mean square error equalization in a spread OFDM wireless communication system, as claimed in claim 19.

In one aspect, the present invention provides a new, efficient yet simple, low complexity decoding algorithm for an enhanced OFDM modulator.

Preferably the OFDM modulator is based on a Walsh-Hadamard transform, allowing exploitation of the mathematical properties of a Walsh-Hadamard precoder.

In one form, the new decoding algorithm consists in splitting a received block into two equal parts, one of the parts being decoded first and then subtracted from the received vector to suppress part of the interference and the other of the parts being decoded next. This iterative procedure can be further extended by successive

block splitting and results in a multi-resolution decoding algorithm. An attractive property of this algorithm is that although it still relies on the computation of pseudo-inverses, the expressions of these pseudo-inverses are easy to derive and consist simply in the product of a diagonal matrix by a Walsh Hadamard transform. Thus, using Walsh Hadamard spreading sequences, the inherent complexity penalty of a V-BLAST decoding schemes is simply removed. This allows a significant gain in performance (e.g., around 3-4dB compared to MMSE SOFDM) with only a modest increase in complexity, which motivates:

i) the use of such new modulation schemes in practice and

ii) their proposal as a solution for future wireless LAN standards.

The following technical merits of the new multi-resolution decoding algorithm can be highlighted:

- Low arithmetical complexity compared to existing SIC BLAST techniques with same or better performance.
- Flexibility and scalability of the method (it is possible to adjust the number of iterations to be performed based on a performance/complexity tradeoff).
- Can be combined into all OFDM standards as a proprietary transmission mode (since it can be viewed as a simple extension of current OFDM systems)
- Yields a significant PER performance enhancement compared to classical OFDM and minimum mean square error (MMSE) SOFDM receivers (e.g., 3dB).

Brief Description of the Drawing(s)

One OFDM single user communication system and decoding algorithm for use therein incorporating the present invention will now be described, by way of example only, with reference to the accompanying drawing(s), in which:

FIG. 1 shows a block schematic diagram of a OFDM-CDMA (spread OFDM) single user communication system;

FIG. 2 shows a blcok schematic representation of the system of FIG. 1 modeled in the frequency domain;

FIG. 3 shows a diagrammatic binary tree representation of the two-stage multi-resolution decoding algorithm used in the system of FIG. 1;

FIG. 4 and FIG. 5 show graphical representations of simulation performance of the multi-resolution decoding algorithm compared with other decoding scenarios under different respective channel profiles in terms of BER (bit error rate) as a function of $\frac{E_b}{N_0}$ (energy per bit / noise energy).

Description of Preferred Embodiment(s)

As will be explained below, the decoding algorithm to be described significantly enhances performance

compared to MMSE equalized SOFDM scheme, with a complexity excess that is marginal compared to V-BLAST decoding strategies.

Consider the dimension $N\times 1$ vector s representing the block of complex valued symbols to be transmitted (each one belonging to a finite alphabet called constellation, e.g., QPSK, QAM, etc.). The overall Spread-OFDM transmission system of interest depicted in FIG. 1 includes, in a transmitter, a spreading matrix module 110, a module 120 providing modulation, a module 130 providing guard interval insertion and parallel-to-serial conversion, and a digital-to-analog converter 140. The transmitter is coupled via a wireless communication channel 150 to a receiver including a mixer and analog-to-digital converter 160, a module 170 providing guard interval suppression and serial-to-parallel conversion, a module 180 providing demodulation, and a module 190 providing demodulation.

The system of FIG. 1 can be modelled directly in the frequency domain as illustrated in FIG. 2 so that the received vector y expresses as:

$$y = HWs + b = Ms + b$$

where:

H is a $N\times N$ diagonal matrix, bearing the complex frequency channel attenuations,

W is a $N\times N$ unitary Walsh Hadamard spreading matrix, whose particular recursive structure is exploited in the decoding algorithm to reduce complexity,

b is a $N\times1$ complex white IID (independent and identically distributed) Gaussian noise vector whose component variance is $E\left[|b_k|^2\right]=\sigma^2$. (E stands here for expectation)

In the following anaysis, H, W and σ^2 are assumed to be known at the receiver by any given classical estimation technique.

The procedure described below deals with the retrieval of the information vector s based on the received vector y which is referred as the equalization step. Instead of using a traditional MMSE equalizer, a specific successive interference cancellation algorithm (termed a 'multi-resolution decoding algorithm') will be described. In the following analysis, $()^h$ is defined as the Hermitian transpose operator and I_N is defined as the NxN identity matrix.

The multi-resolution decoding algorithm is based on the following steps:

(i) Decode the received y vector by an MMSE equalizer followed by a non-linear decision function denoted by $dec()$ (e.g., hard decision demapper, soft decision, etc.) $\hat{s}=dec(G_{MMSE}\, y)$ where $G_{MMSE}=M^h(M\, M^h+\sigma^2 I_N)^{-1}$ (convenient implementations of the product $G_{MMSE}\, y$ are detailed below).

(ii) Split the vector $\hat{s}$ in two equal size $N/2$ parts $\hat{s}=\begin{bmatrix}\hat{s}_1\\ \hat{s}_2\end{bmatrix}$.

(iii) Subtract the second half $\hat{s}_2$ of the vector $\hat{s}$ from the received vector y to remove the interference generated by the first half of s (treating s_2 as if $\hat{s}_2 = s_2$.

(iv) Perform an MMSE equalization of the resulting y_1 half-sized vector by matrix G_1, followed by the decision function *dec()* for obtaining a more reliable estimate $\hat{\hat{s}}_1$ of s_1 than $\hat{s}_1$.

(v) Possibly reiterate the procedure, this time on the first half of $\hat{s}$ for retrieving a better estimate $\hat{\hat{s}}_2$ of s_2 than $\hat{s}_2$.

(vi) These operations can be repeated substituting $\hat{s}_1$ and $\hat{s}_2$ by $\hat{\hat{s}}_1$ and $\hat{\hat{s}}_2$ respectively

Translated into equations, this amounts to the following steps:

First stage (310) of the multi-resolution decoding algorithm

Step 0, (300) : MMSE equalization of $y : \hat{s} = \begin{bmatrix} \hat{s}_1 \\ \hat{s}_2 \end{bmatrix} = dec(G_{MMSE}$ $y)$

Step 1 : $y_1 := y - M \begin{bmatrix} 0 \\ \hat{s}_2 \end{bmatrix} = M \begin{bmatrix} s_1 \\ s_2 - \hat{s}_2 \end{bmatrix} + b$

Step 2 : MMSE equalization of $\hat{\hat{s}}_1$: $\hat{\hat{s}}_1 = dec(G_1^{(1)} y_1)$

Step 3 : $y_2 := y - M \begin{bmatrix} \hat{\hat{s}}_1 \\ 0 \end{bmatrix} = M \begin{bmatrix} s_1 - \hat{\hat{s}}_1 \\ s_2 \end{bmatrix} + b$

Step 4 : MMSE equalization of $\hat{\hat{s}}_2$: $\hat{\hat{s}}_2 = dec(G_2^{(1)} y_2)$

Step 5 : $\hat{s} = \begin{bmatrix} \hat{s}_1 \\ \hat{s}_2 \end{bmatrix} := \begin{bmatrix} \hat{\hat{s}}_1 \\ \hat{\hat{s}}_2 \end{bmatrix}$

Step 6 : go to Step 1

It should be noted that although as stated above only a subdivision by two of the received vector y is performed, in its more generalized form the procedure can apply to smaller subdivisions of y of length N divided by a power of 2: $N/2^k$ for any integer k such that the result remains an integer. The generalized algorithm consists in reiterating the procedure already explained to each resulting sub-block of y. Let stage i of the algorithm define the operations performed for a level of subdivisions of y in blocks of size $N/2^i$.

As an illustration, the second stage of the proposed multi-resolution algorithm results in the following operations:

Second stage (320) of the multi-resolution decoding algorithm

Step 0: form $\hat{s} = \begin{bmatrix} \hat{s}_1 \\ \hat{s}_2 \\ \hat{s}_3 \\ \hat{s}_4 \end{bmatrix}$

Step 1 : $y_1 := y - M\begin{bmatrix} 0 \\ \hat{s}_2 \\ \hat{s}_3 \\ \hat{s}_4 \end{bmatrix} = M\begin{bmatrix} s_1 \\ s_2 - \hat{s}_2 \\ s_3 - \hat{s}_3 \\ s_4 - \hat{s}_4 \end{bmatrix} + b$

Step 2 : MMSE equalization of $\hat{\hat{s}}_1$: $\hat{\hat{s}}_1 = dec(G_1^{(2)} y_1)$

Step 3 : $y_2 := y - M\begin{bmatrix}\hat{\hat{s}}_1\\0\\\hat{s}_3\\\hat{s}_4\end{bmatrix} = M\begin{bmatrix}s_1-\hat{\hat{s}}_1\\s_2\\s_3-\hat{s}_3\\s_4-\hat{s}_4\end{bmatrix}+b$

Step 4 : MMSE equalization of $\hat{\hat{s}}_2$: $\hat{\hat{s}}_2 = dec(G_2^{(2)}y_2)$

Step 5 : $y_3 := y - M\begin{bmatrix}\hat{\hat{s}}_1\\\hat{\hat{s}}_2\\0\\\hat{s}_4\end{bmatrix} = M\begin{bmatrix}s_1-\hat{\hat{s}}_1\\s_2-\hat{\hat{s}}_2\\s_3\\s_4-\hat{s}_4\end{bmatrix}+b$

Step 6 : MMSE equalization of $\hat{\hat{s}}_3$: $\hat{\hat{s}}_3 = dec(G_3^{(2)}y_3)$

Step 7 : $y_4 := y - M\begin{bmatrix}\hat{\hat{s}}_1\\\hat{\hat{s}}_2\\\hat{\hat{s}}_3\\0\end{bmatrix} = M\begin{bmatrix}s_1-\hat{\hat{s}}_1\\s_2-\hat{\hat{s}}_2\\s_3-\hat{\hat{s}}_3\\s_4\end{bmatrix}+b$

Step 8 : MMSE equalization of $\hat{\hat{s}}_4$: $\hat{\hat{s}}_4 = dec(G_4^{(2)}y_4)$

Step 9 : $\hat{s} := \hat{\hat{s}}$

Step 10 : go to Step 1

Note that $G_i^{(\gamma)}$ denotes the MMSE equalizer matrix at stage γ for the sub-block r of vector y of size $N/2^{\gamma}$.

It is important to note that each stage can be sequenced in many ways following the graphic illustration of FIG. 3 using a binary tree. Each path in the binary tree results into another instantiation of the proposed algorithm. The depth in terms of number of stages and the number of times each of the stages has to be iterated can be determined by a complexity/performance trade-off criterion.

Thus in order to refine the decoding, the same mechanisms can be applied to blocks of size *N/4*, and then *N/8*, etc. leading to a higher resolution of the decoding.

Clearly, increasing the number of stages and iterations yields a more robust estimation procedure. However, simulations show that the bit error rate converges after a few iterations, so to improve again the decoded vector, fortunately in practice only the second stage of the algorithm needs to be considered.

A fast algorithm for computing the product of vector y_l by matrix $G_l^{(\gamma)}$ be implemented as follows.

Firstly, the expression of matrices $G_l^{(\gamma)}$ is examined, by fairly assuming that at each stage:

- $E\left([s_k - \hat{s}_k][s_k^H - s_k^H]\right) \approx \rho(p_k) I_{N/2^\gamma}$
- $E(s_k \hat{s}_{k'}) \approx 0$ for $k \neq k'$
- $E(\hat{s}_k b^H) \approx 0$

where E is the expectation operator and ρ is a function of p_k, the bit error probability for the k^{th} block after its last equalization, depending on the constellation used.

Under these assumptions, it is possible to calculate the expression of the MMSE equalization matrix used at each stage:

$$G_k^{(\gamma)} = \left[0_{\frac{N}{2^\gamma} \times \frac{(k-1)N}{2^\gamma}} \quad I_{\frac{N}{2^\gamma}} \quad 0_{\frac{N}{2^\gamma} \times \frac{(2^\gamma - k)N}{2^\gamma}} \right] M^H \left(M D_k^{(\gamma)} M + \sigma^2 I_N \right)^{-1}$$

where $D_k^{(\gamma)}$ is the following block-diagonal matrix :

$$D_k^{(\gamma)} = diag\left(\rho(p_1) I_{\frac{N}{2^\gamma}} \quad \cdots \quad \rho(p_{k-1}) I_{\frac{N}{2^\gamma}} \quad I_{\frac{N}{2^\gamma}} \quad \rho(p_{k+1}) I_{\frac{N}{2^\gamma}} \quad \cdots \quad \rho(p_{2^\gamma}) I_{\frac{N}{2^\gamma}} \right)$$

Simulations show that the terms $\rho(p_k)$ do not play an important role in overall performance, and thus can be neglected (replaced by 0), which greatly simplifies the calculus of the matrix products. It can be shown that in this case, when defining the $\frac{N}{2^\gamma} \times \frac{N}{2^\gamma}$ diagonal matrix:

$$\Delta_\gamma = diag\left\{ \frac{1}{\sigma^2 + \frac{1}{2^\gamma} \sum_{k=0}^{2^\gamma - 1} \left| h_{l+kN/2^\gamma} \right|^2} \right\}_{l=1}^{N/2^\gamma}$$

the following general result is obtained:

$$\begin{bmatrix} G_1^{(\gamma)} \\ \cdots \\ G_{2^\gamma}^{(\gamma)} \end{bmatrix} = W \begin{bmatrix} \Delta_\gamma & 0 & 0 \\ 0 & \cdots & 0 \\ 0 & 0 & \Delta_\gamma \end{bmatrix} H^*$$

Thus the product by $G_i^{(\gamma)}$ reduces simply to the product of y_i by a diagonal matrix depending on the channel coefficients (computed and stored once only) followed by the products of a subset of a Walsh-Hadamard matrix of size $\frac{N}{2^\gamma} \times N$. Therefore, the procedure detailed in the two previous equations results in a simple low arithmetical complexity way for performing the various MMSE equalizations steps. Instead of the expected heavy arithmetic complexity order of N^3 required by the

$G_i^{(\gamma)}$ product, a much simpler complexity of order $2^\gamma N \log_2\left(\frac{N}{2^\gamma}\right)$ at each stage results.

The complexity of the multi-resolution decoding algorithm described above can be estimated as follows. The arithmetical simplifications due to the Walsh-Hadamard structure lead to quite a low complexity. At each stage γ of the algorithm, the complexity $C(\gamma, N)$ of one iteration (i.e., 2^γ calculus of y, of $G_i^{(\gamma)} y$ and decisions) can be overestimated:

$$C(\gamma,N) \approx N\left(2^\gamma\left(2\log_2\left(\frac{N}{2^\gamma}\right)+6\right)+2+\frac{3}{2^\gamma}\right)\times AddR + N\left(3\times 2^\gamma+4+\frac{5}{2^\gamma}\right)\times MulR + N\times Decisio$$

where $AddR$ is the complexity of an addition of two real values (assumed equal to that of a subtraction), $MulR$ is the complexity of a multiplication, and $Decision$ is the complexity of a hard decision on a complex value (the choice of a symbol).

There follows an illustration of the performance improvement provided by the above-described multi-resolution decoding algorithm in the context of a 5.2GHz, 20MHz bandwidth, 64 carrier with 800ns guard time HIPERLAN/2 OFDM system using a QPSK constellation. Simulations were run using 2 channel profiles: (i) a perfect time interleaved BRAN 'E' channel model, and (ii) pure independent Rayleigh fadings in the frequency domain. The results in terms of bit error rate (BER) for uncoded scenarios as a

function of the ratio $\frac{E_b}{N_0}$ (energy per bit / noise energy) are provided FIG. 4 and FIG. 5.

A clear improvement can be observed by applying our decoding strategy over OFDM and MMSE SOFDM systems using a Walsh-Hadamard spreading sequence: for a target BER of 10^{-4}, more than 3dB is gained by compared to MMSE SOFDM applying one or two iterations at the three first stages.

This means that for the same fixed BER and a given C/I (carrier to interference), 16QAM SOFDM with multiresolution decoding would have the same performance of a QPSK SOFDM MMSE transmission scheme while providing an enhancement of 4 times in bit rate. Such a significant improvement illustrates how improved decoding schemes for existing systems can translate directly in greater system capacity under a given QoS constraint.

It will be understood that the multi-resolution decoding algorithm for OFDM-CDMA, spread OFDM single user systems described above provides the following advantages:
The following technical merits of the new multi-resolution decoding algorithm can be highlighted:

- Low arithmetical complexity compared to existing SIC BLAST techniques with same or better performance.
- Flexibility and scalability of the method (it is possible to adjust the number of iterations to be performed based on a performance/complexity tradeoff).

- Can be combined into all OFDM standards as a proprietary transmission mode (since it can be viewed as a simple extension of current OFDM systems).
- Yields a significant PER performance enhancement compared to classical OFDM and minimum mean square error (MMSE) SOFDM receivers (e.g., 3dB).

Claims

1. A spread OFDM wireless communication system comprising:

at a transmitter

means for transmitting a spread OFDM signal;

at a receiver

means for receiving the spread OFDM signal;

means for equalizing the spread OFDM signal

means for splitting the equalized spread OFDM signal into a first plurality of portions including a first portion and a second portion;

means for making a decision on the second portion

means for subtracting the second portion from the received spread OFDM signal to produce a first difference signal; and

means for processing/equalizing the first difference signal to recover the first portion of the received signal in which interference due to the second portion interfering terms is substantially reduced.

2. The system of claim 1 further comprising:

at the receiver

means for making a decision on the first portion

means for subtracting the first portion from the received spread OFDM signal to produce a second difference signal; and

means for processing/equalizing the second difference signal to recover the second portion

of the received signal in which interference due to the first portion interfering terms is substantially reduced.

Means for iterating the process a certain number of times (described in claim 1 and 2) with the new estimates

3. The system of claim 1 or 2 further comprising: at the receiver

means for splitting the recovered received signal into a second plurality of portions greater in number than the first plurality of portions and including a first subsequent portion, a second subsequent portion, a third subsequent portion and a fourth subsequent portion;

means for subtracting the second, third and fourth subsequent portions from the received signal to produce a first subsequent difference signal; and

means for processing the first subsequent difference signal to recover the first subsequent portion of the recovered received signal in which interference due to the second, third and fourth portion interfering terms is substantially reduced.

Means for making a decision on the first portion

means for subtracting the first, third and fourth subsequent portions from the received

signal to produce a second subsequent difference signal; and

means for processing the second subsequent difference signal to recover the second subsequent portion of the recovered received signal in which interference due to the first, third and fourth portion interfering terms is substantially reduced.

Means for making a decision on the second portion

means for subtracting the first, second and fourth subsequent portions from the received signal to produce a third subsequent difference signal; and

means for processing the third subsequent difference signal to recover the third subsequent portion of the recovered received signal in which interference due to the first, second and fourth portion interfering terms is substantially reduced.

Means for making a decision on the third portion

means for subtracting the first, second and third subsequent portions from the received signal to produce a fourth subsequent difference signal; and

means for processing the fourth subsequent difference signal to recover the fourth

subsequent portion of the recovered received signal in which interference due to the first, second and third portion interfering terms is substantially reduced.

Means for making a decision on the fourth portion

Means for iterating the process of claim 3 .

Means for conducting the same algorithm described in claim 3 with a number of portions multiple of 2.

4. The system of claim 1,2 and 3 wherein the means for performing interference/equalization comprises:

first matrix multiplication means for multiplying by a first diagonal matrix having elements dependent on channel coefficients; and

second matrix multiplication means for multiplying by a second matrix which is a subset of a Walsh Hadamard matrix.

5. The system of claim 1, 2, 3 or 4 wherein the means for processing comprises means for performing minimum mean square error equalization.

6. The system of any preceding claim wherein the means for transmitting a spread OFDM signal comprises means for spreading by performing a Walsh Hadamard transform.

7. A spread OFDM wireless communication system comprising:

at a transmitter

means for transmitting a spread OFDM signal;

at a receiver

means for performing minimum mean square error equalization having:

first matrix multiplication means for multiplying by a first diagonal matrix having elements dependent on channel coefficients; and

second matrix multiplication means for multiplying by a second matrix which is a subset of a Walsh Hadamard matrix.

8. A receiver for use in a spread OFDM wireless communication system, the receiver comprising:

means for receiving a wireless spread OFDM signal;

means for splitting the received spread OFDM signal into a first plurality of portions including a first portion and a second portion;

means for subtracting the second portion from the received spread OFDM signal to produce a first difference signal; and

means for processing the first difference signal to recover the first portion of the received signal in which of interference is substantially removed.

9. The receiver of claim 8 further comprising:

means for subtracting the first portion from the received spread OFDM signal to produce a second difference signal; and

means for processing the second difference signal to recover the second portion of the received signal in which interference is substantially removed.

10. The receiver of claim 8 or 9 further comprising:

means for splitting the recovered received signal into a second plurality of portions greater in number than the first plurality of portions and including a first subsequent portion and a second subsequent portion;

means for subtracting the second subsequent portion from the recovered received signal to

produce a first subsequent difference signal; and

means for processing the first subsequent difference signal to recover the first subsequent portion of the recovered received signal in which interference is substantially removed.

11. The receiver of claim 8, 9 or 10 wherein the means for processing comprises means for performing minimum mean square error equalization.

12. The receiver of claim 11 wherein the means for performing minimum mean square error equalization comprises:

first matrix multiplication means for multiplying by a first diagonal matrix having elements dependent on channel coefficients; and

second matrix multiplication means for multiplying by a second matrix which is a subset of a Walsh Hadamard matrix.

13. A receiver for use in a spread OFDM wireless communication system, the receiver comprising:

means for performing minimum mean square error equalization having:

first matrix multiplication means for multiplying by a first diagonal matrix having elements dependent on channel coefficients; and second matrix multiplication means for multiplying by a second matrix which is a subset of a Walsh Hadamard matrix.

14. A method of operating a receiver in a spread OFDM wireless communication method comprising:

receiving a wireless spread OFDM signal;

splitting the received spread OFDM signal into a first plurality of portions including a first portion and a second portion;

subtracting the second portion from the received spread OFDM signal to produce a first difference signal; and

processing the first difference signal to recover the first portion of the received signal in which of interference is substantially removed.

15. The method of claim 14 further comprising:

subtracting the first portion from the received spread OFDM signal to produce a second difference signal; and

processing the second difference signal to recover the second portion of the received signal in which interference is substantially removed.

16. The method of claim 14 or 15 further comprising:

splitting the recovered received signal into a second plurality of portions greater in number than the first plurality of portions and including a first subsequent portion and a second subsequent portion;

subtracting the second subsequent portion from the recovered received signal to produce a first subsequent difference signal; and

processing the first subsequent difference signal to recover the first subsequent portion of the recovered received signal in which interference is substantially removed.

17. The method of claim 14, 15 or 16 wherein the step of processing comprises performing minimum mean square error equalization.

18. The method of claim 17 wherein the step of performing minimum mean square error equalization comprises:

multiplying by a first diagonal matrix having elements dependent on channel coefficients; and

multiplying by a second matrix which is a subset of a Walsh Hadamard matrix.

19. A method for performing minimum mean square error equalization in a spread OFDM wireless communication system, the method comprising:

multiplying by a first diagonal matrix having elements dependent on channel coefficients; and multiplying by a second matrix which is a subset of a Walsh Hadamard matrix.

Abstract

SYSTEM, RECEIVER AND METHOD OF OPERATION FOR SPREAD OFDM WIRELESS COMMUNICATION

A system (110-190), receiver (160-190) and method of operation for spread OFDM wireless communication (single user OFDM-CDMA with cyclic-prefix) by:
Equalizing the splitting received spread OFDM signal (y) Splitting the equalized received spread OFDM signal (y) into first and second portions ($\hat{s}_1$, $\hat{s}_2$); making a decision on the second portion and subtracting the second portion from the received spread OFDM signal to produce a first difference signal; processing the first difference signal to recover the first portion of the received signal in which of the symbol interfering terms of the second portion are substantially reduced; making a decision and subtracting the first portion from the received spread OFDM signal to produce a second difference signal; and processing the second difference signal to recover the second portion of the received signal in which the symbol interfering terms of the first portion are substantially reduced. The process is iterated extensively at this stage. In a second stage, the recovered received signal is split into a greater number of portions (e.g., 4), and processed similarly to further reduce interference. The same mechanisms can be applied to blocks of reduced size divided by 8,16 etc.) leading to a higher resolution of the decoding and a tree-like structure.
Also, minimum mean square error equalization is performed by multiplying by a first diagonal matrix having elements dependent on channel coefficients; and multiplying by a

second matrix which is a subset of a Walsh Hadamard matrix.

This provides low arithmetical complexity, it is possible to adjust the number of iterations to be performed based on a performance/complexity tradeoff, it can be viewed as a simple extension of current OFDM systems, and it yields a significant PER performance enhancement (e.g., 3dB).

Figs 1 & 2

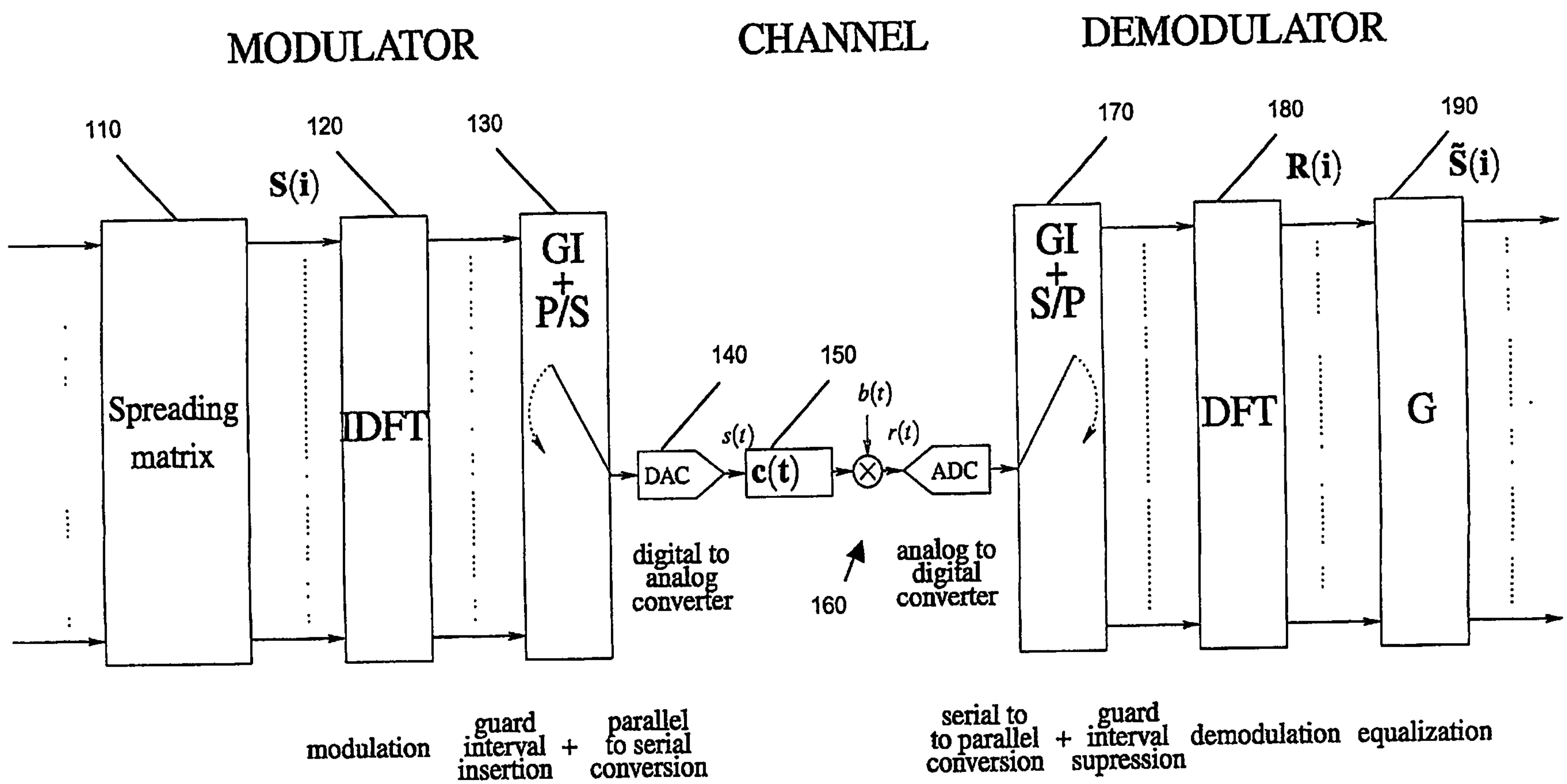
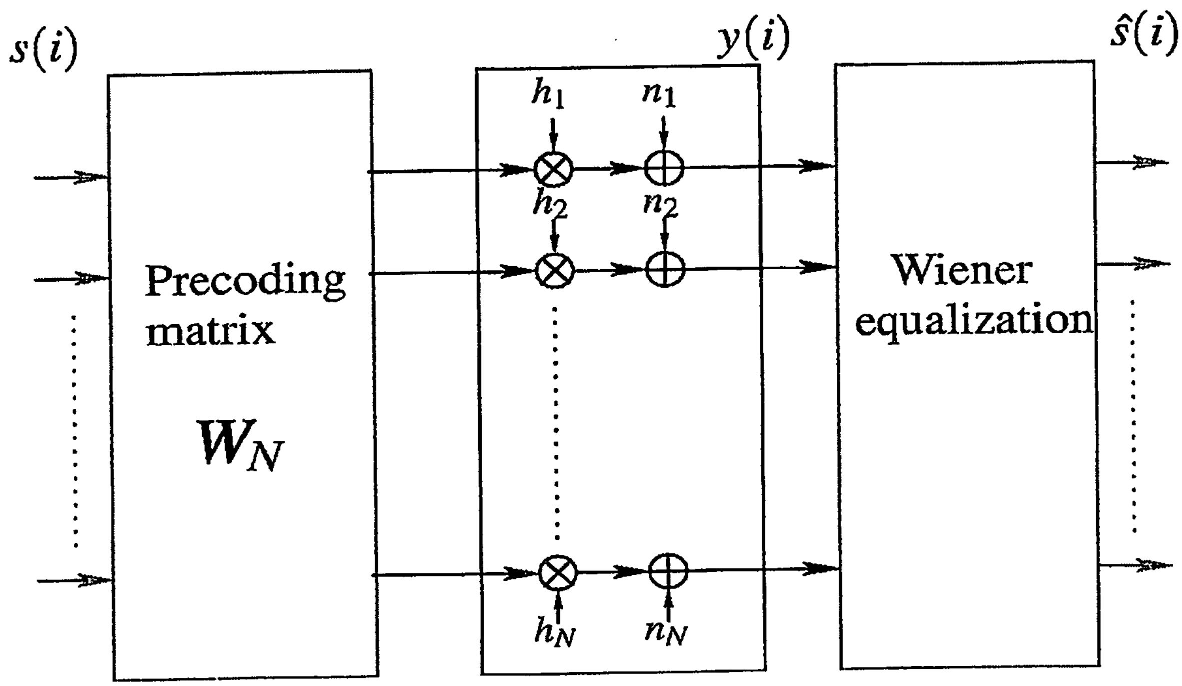

MODULATOR
CHANNEL
DEMODULATOR
110
120
130
140
150
160
170
180
190
S(i)
R(i)
S̃(i)
Spreading matrix
IDFT
GI + P/S
DAC
s(t)
c(t)
b(t)
r(t)
ADC
GI + S/P
DFT
G
digital to analog converter
analog to digital converter
modulation
guard interval insertion + parallel to serial conversion
serial to to parallel conversion + guard interval supression
demodulation
equalization

FIG. 1



$s(i)$
Precoding matrix
W_N
h_1
n_1
h_2
n_2
h_N
n_N
$y(i)$
Wiener equalization
$\hat{s}(i)$

FIG. 2

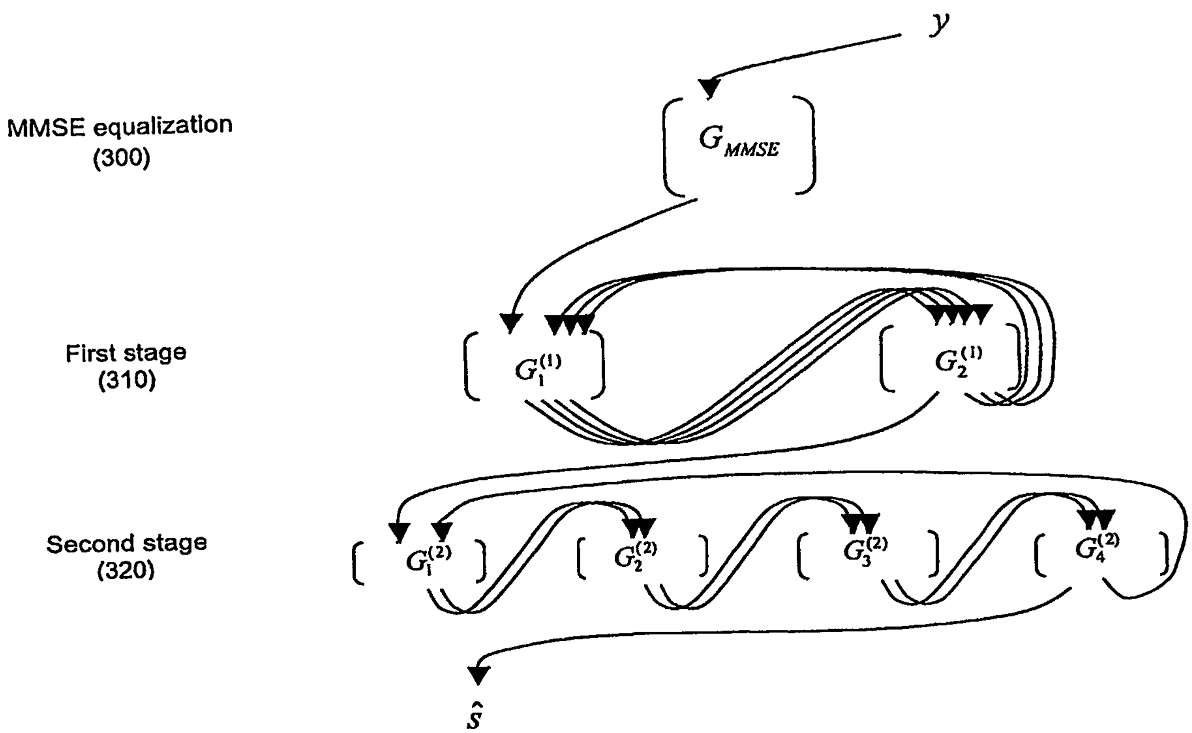
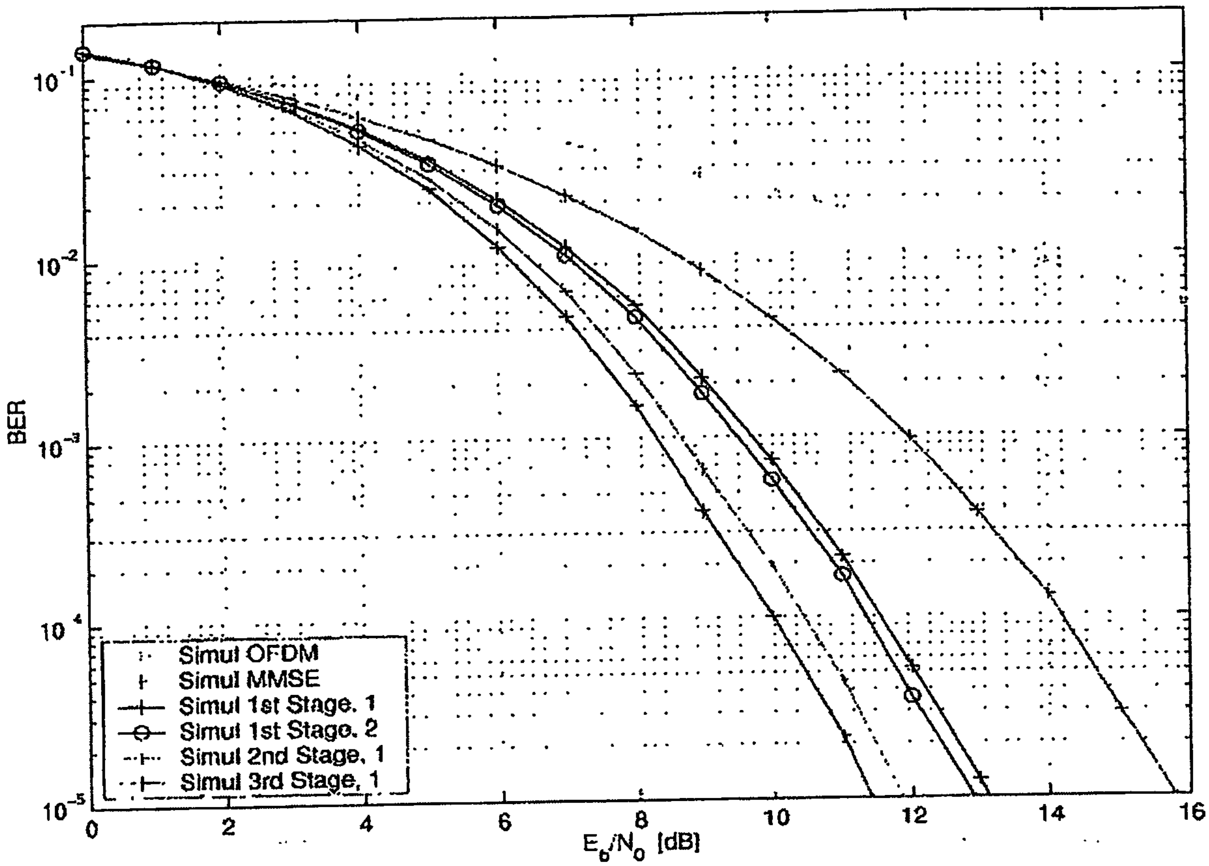

y
MMSE equalization
(300)
G_{MMSE}
First stage
(310)
$G_1^{(1)}$
$G_2^{(1)}$
Second stage
(320)
$G_1^{(2)}$
$G_2^{(2)}$
$G_3^{(2)}$
$G_4^{(2)}$
$\hat{s}$

FIG. 3



BER
10^{-1}
10^{-2}
10^{-3}
10^{-4}
10^{-5}
0
2
4
6
8
10
12
14
16
E_b/N_0 [dB]
Simul OFDM
Simul MMSE
Simul 1st Stage. 1
Simul 1st Stage. 2
Simul 2nd Stage. 1
Simul 3rd Stage. 1

FIG. 4

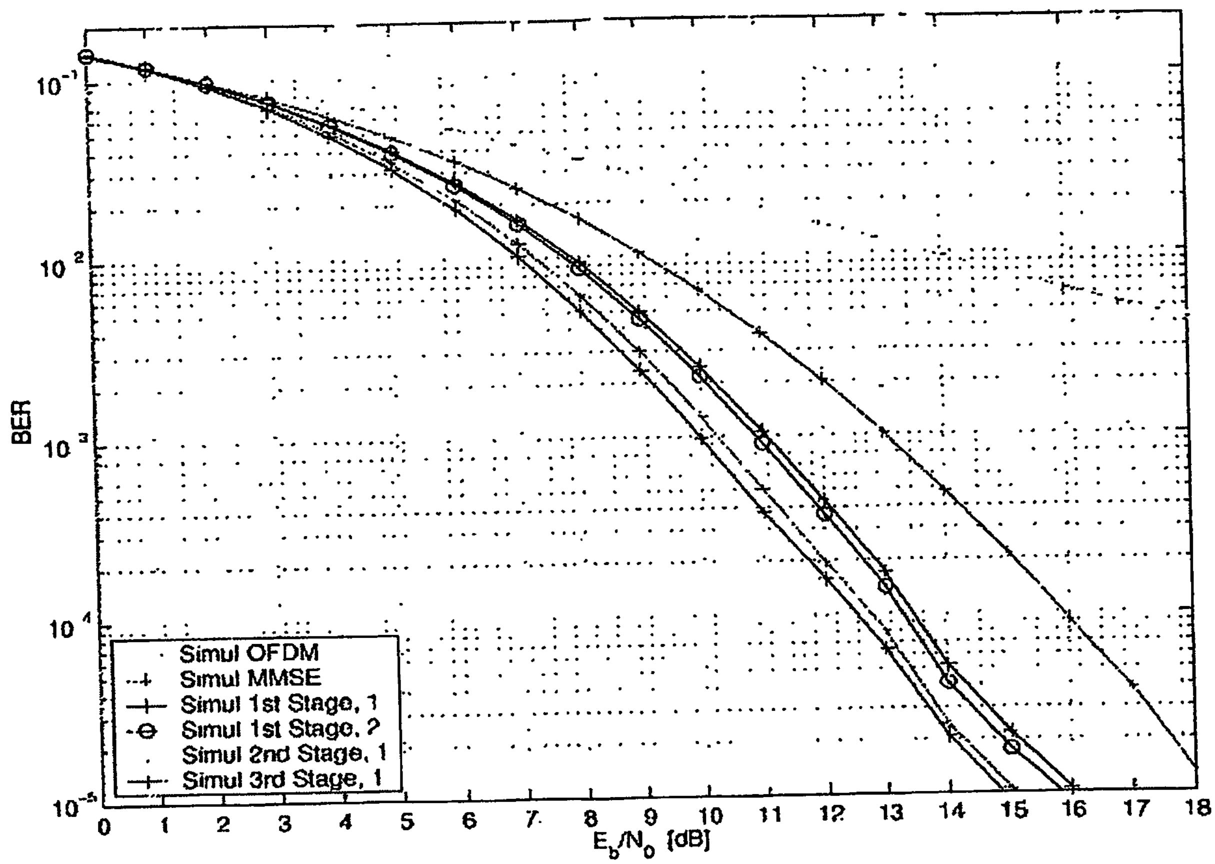

BER
10^{-1}
10^{-2}
10^{-3}
10^{-4}
10^{-5}
0 1 2 3 4 5 6 7 8 9 10 11 12 13 14 15 16 17 18
E_b/N_0 [dB]
Simul OFDM
Simul MMSE
Simul 1st Stage, 1
Simul 1st Stage, 2
Simul 2nd Stage, 1
Simul 3rd Stage, 1

FIG. 5

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